

## FEATURES

**4 ns propagation delay at 5 V**  
**Single-supply operation: 3 V to 5 V**  
**100 MHz input**  
**Latch function**

## APPLICATIONS

**High speed timing**  
**Clock recovery and clock distribution**  
**Line receivers**  
**Digital communications**  
**Phase detectors**  
**High speed sampling**  
**Read channel detection**  
**PCMCIA cards**  
**Zero-crossing detector**  
**High speed analog-to-digital converter (ADC)**  
**Upgrade for LT1394 and LT1016 designs**

## GENERAL DESCRIPTION

The AD8611/AD8612 are single and dual 4 ns comparators with latch function and complementary output. The latch is not functional if  $V_{CC}$  is less than 4.3 V.

Fast 4 ns propagation delay makes the AD8611/AD8612 good choices for timing circuits and line receivers. Propagation delays for rising and falling signals are closely matched and tracked over temperature. This matched delay makes the AD8611/AD8612 good choices for clock recovery because the duty cycle of the output matches the duty cycle of the input.

## PIN CONFIGURATIONS

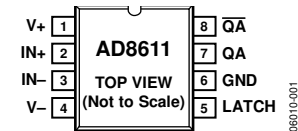


Figure 1. 8-Lead Narrow Body SOIC (R-8)

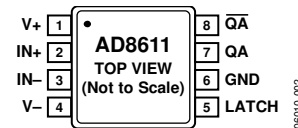


Figure 2. 8-Lead MSOP (RM-8)

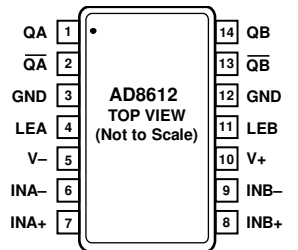


Figure 3. 14-Lead TSSOP (RU-14)

The AD8611 has the same pinout as the LT1016 and LT1394, with lower supply current and a wider common-mode input range, which includes the negative supply rail.

The AD8611/AD8612 are specified over the industrial temperature range ( $-40^{\circ}\text{C}$  to  $+85^{\circ}\text{C}$ ). The AD8611 is available in both 8-lead MSOP and narrow 8-lead SOIC surface-mount packages. The AD8612 is available in a 14-lead TSSOP surface-mount package.

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## REVISION HISTORY

### 12/2016—Rev. A to Rev. B

Changes to Input Voltage Parameter, Table 3 .....	5
Added Input Current Parameter, Table 3 .....	5
Deleted Endnote 1, Table 3.....	5
Updated Outline Dimensions .....	17
Changes to Ordering Guide .....	18

### 8/2006—Rev. 0 to Rev. A

Updated Format.....	Universal
Added No Latch if $V_{CC} < 4.3$ V .....	Universal
Changes to Pin Names .....	Universal
Added Pin Configurations and Function Descriptions Page .....	6
Changes to Table 8.....	12
Changes to Figure 26.....	12
Changes to Ordering Guide .....	17

### 4/2000—Revision 0: Initial Version

## SPECIFICATIONS

$V_+ = 5.0\text{ V}$ ,  $V_- = V_{\text{GND}} = 0\text{ V}$ ,  $T_A = 25^\circ\text{C}$ , unless otherwise noted.

Table 1.

Parameter	Symbol	Test Conditions/Comments	Min	Typ	Max	Unit
<b>INPUT CHARACTERISTICS</b>						
Offset Voltage	$V_{\text{OS}}$	$-40^\circ\text{C} \leq T_A \leq +85^\circ\text{C}$		1	7	mV
Offset Voltage Drift	$\Delta V_{\text{OS}}/\Delta T$			4	8	$\mu\text{V}/^\circ\text{C}$
Input Bias Current	$I_{\text{B}}$	$V_{\text{CM}} = 0\text{ V}$	-6	-4		$\mu\text{A}$
	$I_{\text{B}}$	$-40^\circ\text{C} \leq T_A \leq +85^\circ\text{C}$	-7	-4.5		$\mu\text{A}$
Input Offset Current	$I_{\text{OS}}$	$V_{\text{CM}} = 0\text{ V}$			$\pm 4$	$\mu\text{A}$
Input Common-Mode Voltage Range	$V_{\text{CM}}$		0.0		3.0	V
Common-Mode Rejection Ratio	CMRR	$0\text{ V} \leq V_{\text{CM}} \leq 3.0\text{ V}$	55	85		dB
Large Signal Voltage Gain	$A_{\text{VO}}$	$R_{\text{L}} = 10\text{ k}\Omega$		3000		V/V
Input Capacitance	$C_{\text{IN}}$			3.0		pF
<b>LATCH ENABLE INPUT</b>						
Logic 1 Voltage Threshold	$V_{\text{IH}}$	$V_{\text{CC}} > 4.3\text{ V}$	2.0	1.65		V
Logic 0 Voltage Threshold	$V_{\text{IL}}$	$V_{\text{CC}} > 4.3\text{ V}$		1.60	0.8	V
Logic 1 Current	$I_{\text{IH}}$	$V_{\text{CC}} > 4.3\text{ V}$ , $V_{\text{LH}} = 3.0\text{ V}$	-1.0	-0.3		$\mu\text{A}$
Logic 0 Current	$I_{\text{IL}}$	$V_{\text{CC}} > 4.3\text{ V}$ , $V_{\text{LL}} = 0.3\text{ V}$	-5	-2.7		$\mu\text{A}$
Latch Enable						
Pulse Width	$t_{\text{PW(E)}}$	$V_{\text{CC}} > 4.3\text{ V}$		3		ns
Setup Time	$t_{\text{S}}$	$V_{\text{CC}} > 4.3\text{ V}$		0.5		ns
Hold Time	$t_{\text{H}}$	$V_{\text{CC}} > 4.3\text{ V}$		0.5		ns
<b>DIGITAL OUTPUTS</b>						
Logic 1 Voltage	$V_{\text{OH}}$	$I_{\text{OH}} = 50\text{ }\mu\text{A}$ , $\Delta V_{\text{IN}} > 250\text{ mV}$	3.0	3.35		V
Logic 1 Voltage	$V_{\text{OH}}$	$I_{\text{OH}} = 3.2\text{ mA}$ , $\Delta V_{\text{IN}} > 250\text{ mV}$	2.4	3.4		V
Logic 0 Voltage	$V_{\text{OL}}$	$I_{\text{OL}} = 3.2\text{ mA}$ , $\Delta V_{\text{IN}} > 250\text{ mV}$		0.25	0.4	V
<b>DYNAMIC PERFORMANCE</b>						
Input Frequency	$f_{\text{MAX}}$	400 mV p-p sine wave		100		MHz
Propagation Delay	$t_{\text{P}}$	200 mV step with 100 mV overdrive <sup>1</sup>		4.0	5.5	ns
		$-40^\circ\text{C} \leq T_A \leq +85^\circ\text{C}$		5		ns
Propagation Delay	$t_{\text{P}}$	100 mV step with 5 mV overdrive		5		ns
Differential Propagation Delay (Rising Propagation Delay vs. Falling Propagation Delay)	$\Delta t_{\text{P}}$	100 mV step with 100 mV overdrive <sup>1</sup>		0.5	2.0	ns
Rise Time		20% to 80%		2.5		ns
Fall Time		80% to 20%		1.1		ns
<b>POWER SUPPLY</b>						
Power Supply Rejection Ratio	PSRR	$4.5\text{ V} \leq V_+ \leq 5.5\text{ V}$	55	73		dB
$V_+$ Supply Current <sup>2</sup>	$I_+$	$-40^\circ\text{C} \leq T_A \leq +85^\circ\text{C}$		5.7	10	mA
					10	
Ground Supply Current <sup>2</sup>	$I_{\text{GND}}$	$V_{\text{O}} = 0\text{ V}$ , $R_{\text{L}} = \infty$		3.5	7	mA
		$-40^\circ\text{C} \leq T_A \leq +85^\circ\text{C}$			7	mA
$V_-$ Supply Current <sup>2</sup>	$I_-$	$-40^\circ\text{C} \leq T_A \leq +85^\circ\text{C}$		2.2	4	mA
					5	mA

<sup>1</sup> Guaranteed by design.

<sup>2</sup> Per comparator.

$V_+ = 3.0\text{ V}$ ,  $V_- = \text{VGND} = 0\text{ V}$ ,  $T_A = 25^\circ\text{C}$ , unless otherwise noted.

**Table 2.**

Parameter	Symbol	Test Conditions/Comments	Min	Typ	Max	Unit
<b>INPUT CHARACTERISTICS</b>						
Offset Voltage	$V_{OS}$			1	7	mV
Input Bias Current	$I_B$	$V_{CM} = 0\text{ V}$	-6	-4.0		$\mu\text{A}$
	$I_B$	$-40^\circ\text{C} \leq T_A \leq +85^\circ\text{C}$	-7	-4.5		$\mu\text{A}$
Input Common-Mode Voltage Range	$V_{CM}$		0		1.0	V
Common-Mode Rejection Ratio	CMRR	$0\text{ V} \leq V_{CM} \leq 1.0\text{ V}$	55			dB
<b>OUTPUT CHARACTERISTICS</b>						
Output High Voltage	$V_{OH}$	$I_{OH} = -3.2\text{ mA}$ , $V_{IN} > 250\text{ mV}$	1.2 <sup>1</sup>			V
Output Low Voltage	$V_{OL}$	$I_{OL} = +3.2\text{ mA}$ , $V_{IN} > 250\text{ mV}$			0.3	V
<b>LATCH ENABLE INPUT</b>						
		Not functional if $V_{CC} < 4.3\text{ V}$				
<b>POWER SUPPLY</b>						
Power Supply Rejection Ratio	PSRR	$2.7\text{ V} \leq V_+ \leq 6\text{ V}$		46		dB
Supply Currents		$V_O = 0\text{ V}$ , $R_L = \infty$				
$V_+$ Supply Current <sup>2</sup>	$I_+$	$-40^\circ\text{C} \leq T_A \leq +85^\circ\text{C}$		4.5	6.5	mA
					10	mA
Ground Supply Current <sup>2</sup>	$I_{GND}$	$-40^\circ\text{C} \leq T_A \leq +85^\circ\text{C}$		2.5	3.5	mA
					5.5	mA
$V_-$ Supply Current <sup>2</sup>	$I_-$	$-40^\circ\text{C} \leq T_A \leq +85^\circ\text{C}$		2	3.5	mA
					4.8	mA
<b>DYNAMIC PERFORMANCE</b>						
Propagation Delay	$t_P$	100 mV step with 20 mV overdrive <sup>3</sup>		4.5	6.5	ns

<sup>1</sup> Output high voltage without pull-up resistor. It can be useful to have a pull-up resistor to  $V_+$  for 3 V operation.

<sup>2</sup> Per comparator.

<sup>3</sup> Guaranteed by design.

## ABSOLUTE MAXIMUM RATINGS

Table 3.

Parameter	Rating
Total Analog Supply Voltage	7.0 V
Digital Supply Voltage	7.0 V
Input Voltage	VCC +0.3 V to VEE -0.3 V
Differential Input Voltage	±5 V
Output Short-Circuit Duration to GND	Indefinite
Input Current	±5 mA
Storage Temperature Range	
R, RU, RM Packages	-65°C to +150°C
Operating Temperature Range	-40°C to +85°C
Junction Temperature Range	
R, RU, RM Packages	-65°C to +150°C
Lead Temperature Range (Soldering, 10 sec)	300°C

Stresses at or above those listed under Absolute Maximum Ratings may cause permanent damage to the product. This is a stress rating only; functional operation of the product at these or any other conditions above those indicated in the operational section of this specification is not implied. Operation beyond the maximum operating conditions for extended periods may affect product reliability.

## THERMAL RESISTANCE

Table 4.

Package Type	$\theta_{JA}^1$	$\theta_{JC}$	Unit
8-Lead SOIC (R)	158	43	°C/W
8-Lead MSOP (RM)	240	43	°C/W
14-Lead TSSOP (RU)	240	43	°C/W

<sup>1</sup> $\theta_{JA}$  is specified for the worst-case conditions, that is, a device in socket for P-DIP and a device soldered in circuit board for SOIC and TSSOP.

## ESD CAUTION



**ESD (electrostatic discharge) sensitive device.** Charged devices and circuit boards can discharge without detection. Although this product features patented or proprietary protection circuitry, damage may occur on devices subjected to high energy ESD. Therefore, proper ESD precautions should be taken to avoid performance degradation or loss of functionality.

## PIN CONFIGURATIONS AND FUNCTION DESCRIPTIONS

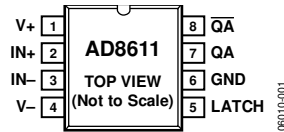


Figure 4. 8-Lead Narrow Body SOIC Pin Configuration

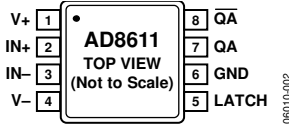


Figure 5. 8-Lead MSOP Pin Configuration

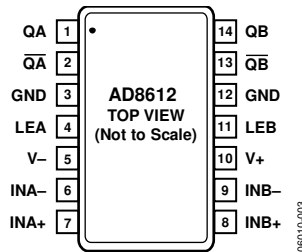


Figure 6. 14-Lead TSSOP Pin Configuration

Table 5. Pin Function Descriptions

Pin No.		Mnemonic	Description
SOIC and MSOP	TSSOP		
1	10	V+	Positive Supply Terminal.
2		IN+	Noninverting Analog Input of the Differential Input Stage.
3		IN-	Inverting Analog Input of the Differential Input Stage.
4	5	V-	Negative Supply Terminal.
5		LATCH	Latch Enable Input.
6	3, 12	GND	Negative Logic Supply
7	1	QA	One of Two Complementary Output for Channel A.
8	2	QA	One of Two Complementary Output for Channel A.
	14	QB	One of Two Complementary Output for Channel B.
	13	QB	One of Two Complementary Output for Channel B.
	4	LEA	Channel A Latch Enable.
	11	LEB	Channel B Latch Enable.
	7	INA+	Noninverting Analog Input of the Differential Input Stage for Channel A.
	6	INA-	Inverting Analog Input of the Differential Input Stage for Channel A.
	8	INB+	Noninverting Analog Input of the Differential Input Stage for Channel B.
	9	INB-	Inverting Analog Input of the Differential Input Stage for Channel B.

### TYPICAL PERFORMANCE CHARACTERISTICS

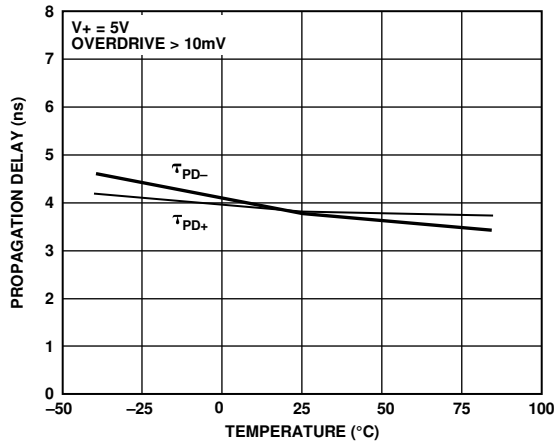


Figure 7. Propagation Delay vs. Temperature

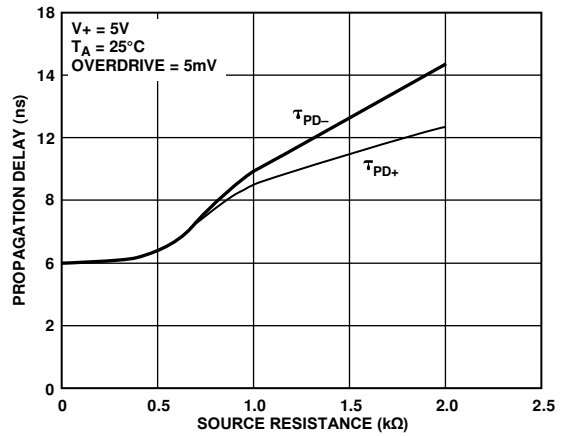


Figure 10. Propagation Delay vs. Source Resistance

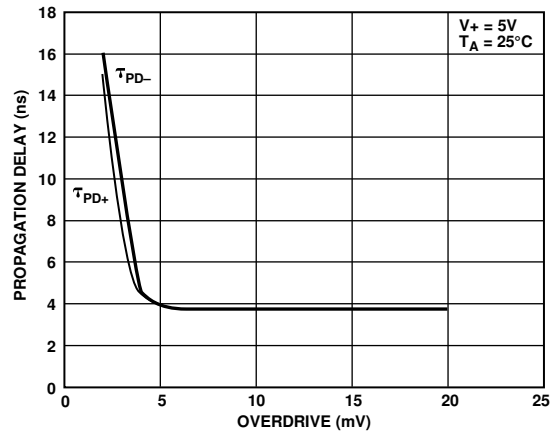


Figure 8. Propagation Delay vs. Overdrive

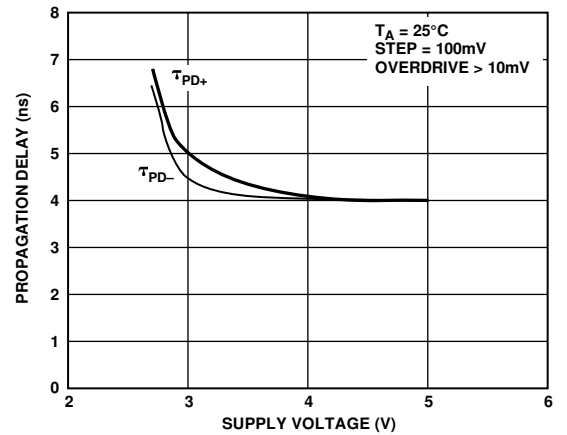


Figure 11. Propagation Delay vs. Supply Voltage

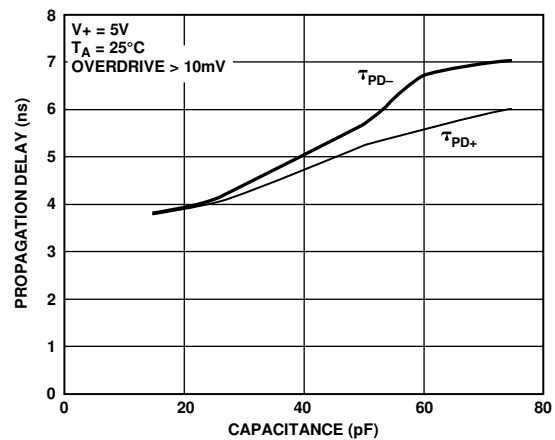


Figure 9. Propagation Delay vs. Load Capacitance

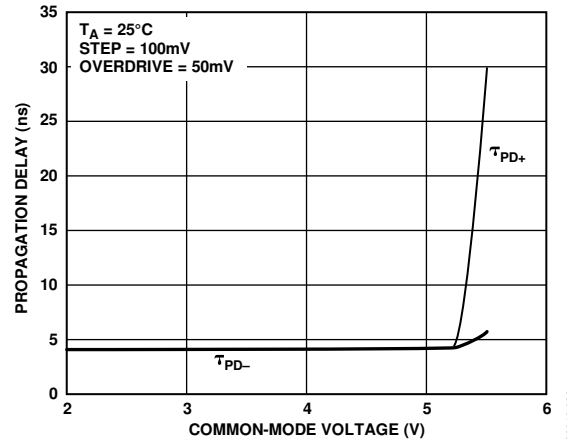


Figure 12. Propagation Delay vs. Common-Mode Voltage

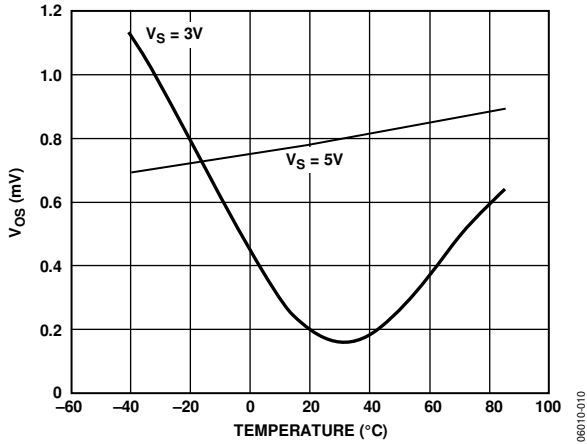


Figure 13. Offset Voltage vs. Temperature

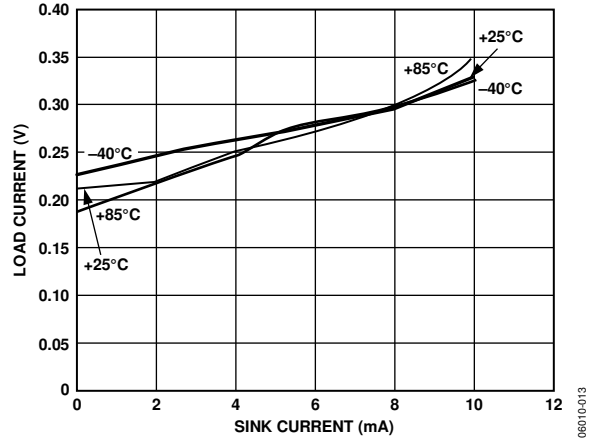


Figure 16. Output Low Voltage vs. Load Current (Sinking) Over Temperature

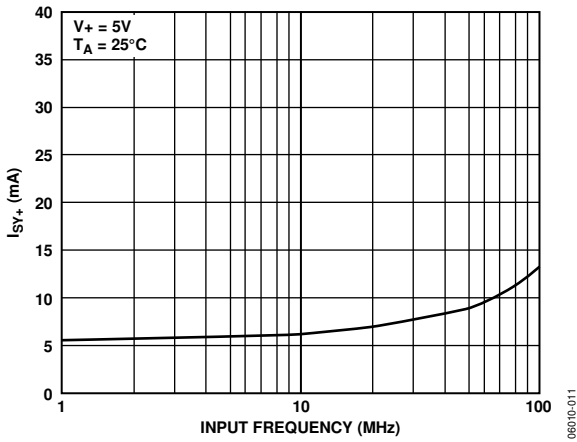


Figure 14. Supply Current vs. Input Frequency

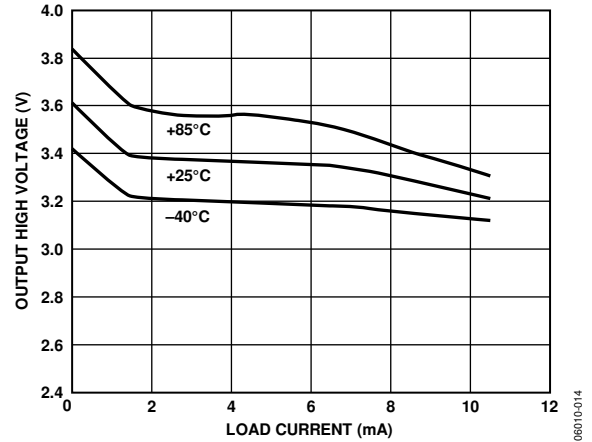


Figure 17. Output High Voltage vs. Load Current (Sourcing) Over Temperature

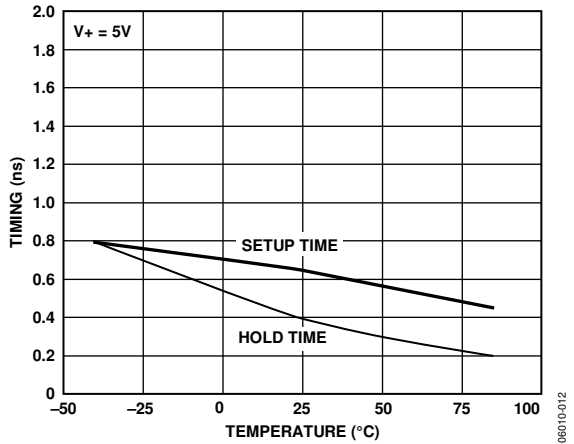


Figure 15. Latch Setup and Hold Time vs. Temperature

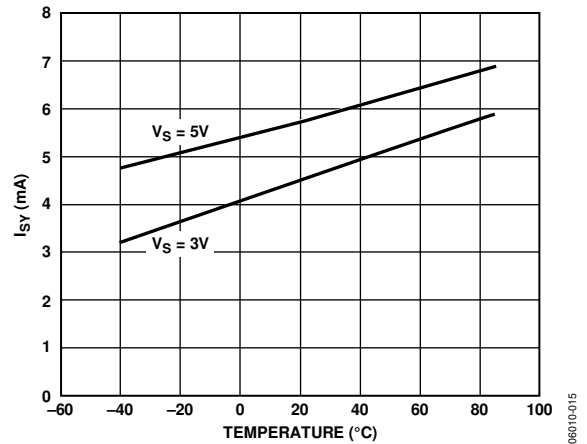


Figure 18. Supply Current vs. Temperature



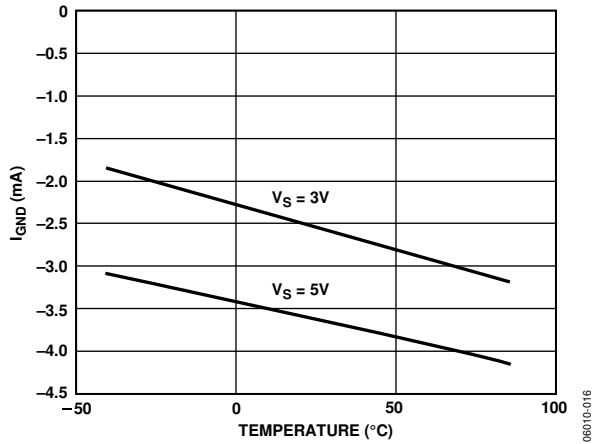


Figure 19. I<sub>GND</sub> vs. Temperature

06610-016

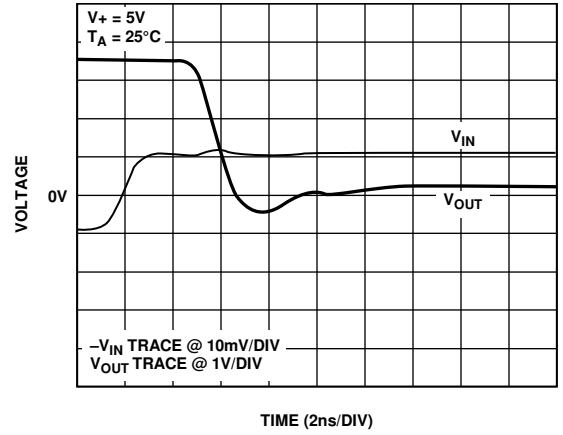


Figure 22. Falling Edge Response

06610-019

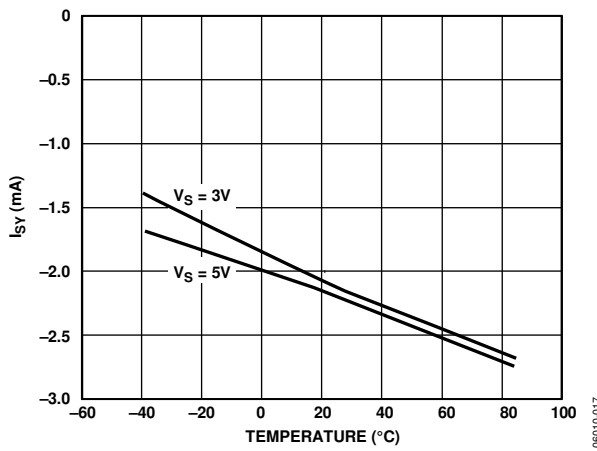


Figure 20. I<sub>SY-</sub> vs. Temperature

06610-017

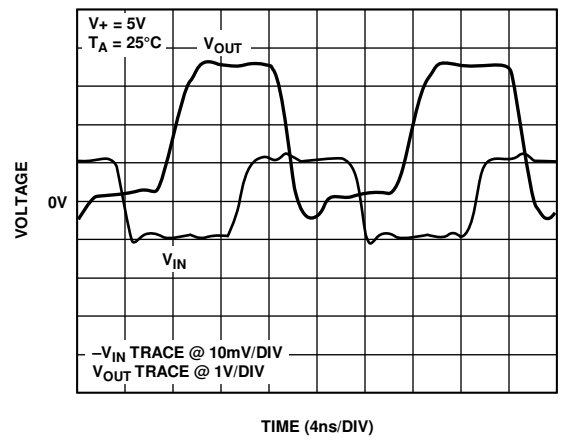


Figure 23. Response to a 50 MHz, 100 mV Input Sine Wave

06610-020

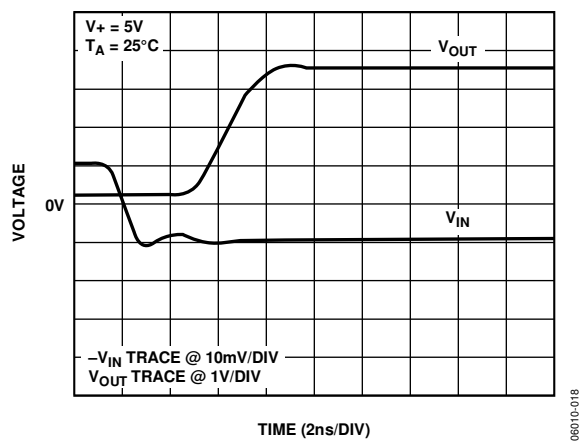


Figure 21. Rising Edge Response

06610-018

## APPLICATIONS INFORMATION

### OPTIMIZING HIGH SPEED PERFORMANCE

As with any high speed comparator or amplifier, proper design and layout of the AD8611/AD8612 must ensure optimal performance. Excess stray capacitance or improper grounding can limit the maximum performance of high speed circuitry.

Minimizing resistance from the source to the comparator input is necessary to minimize the propagation delay of the circuit. Source resistance in combination with the equivalent input capacitance of the AD8611/AD8612 creates an R-C filter that could cause a lagged voltage rise at the input to the comparator. The input capacitance of the AD8611/AD8612 in combination with stray capacitance from an input pin to ground results in several picofarads of equivalent capacitance. Using a surface-mount package and a minimum of input trace length, this capacitance is typically around 3 pF to 5 pF. A combination of 3 k $\Omega$  source resistance and 3 pF of input capacitance yields a time constant of 9 ns, which is slower than the 4 ns propagation delay of the AD8611/AD8612. Source impedances must be less than 1 k $\Omega$  for best performance.

Another important consideration is the proper use of power-supply-bypass capacitors around the comparator. A 1  $\mu$ F bypass capacitor must be placed within 0.5 inches of the device between each power supply pin and ground. Another 10 nF ceramic capacitor must be placed as close as possible to the device in parallel with the 1  $\mu$ F bypass capacitor. The 1  $\mu$ F capacitor reduces any potential voltage ripples from the power supply, and the 10 nF capacitor acts as a charge reservoir for the comparator during high frequency switching.

A continuous ground plane on the PC board is also recommended to maximize circuit performance. A ground plane can be created by using a continuous conductive plane over the surface of the circuit board, only allowing breaks in the plane for necessary traces and vias. The ground plane provides a low inductive current return path for the power supply, thus eliminating any potential differences at various ground points throughout the circuit board caused from ground bounce. A proper ground plane can also minimize the effects of stray capacitance on the circuit board.

### UPGRADING THE LT1394 AND LT1016

The AD8611 single comparator is pin-for-pin compatible with the LT1394 and LT1016 and offers an improvement in propagation delay over both comparators. These devices can easily be replaced with the higher performance AD8611; however, there are differences, so it is useful to ensure that the system still operates properly.

The five major differences between the AD8611 and the LT1016 include input voltage range, input bias currents, propagation delay, output voltage swing, and power consumption. Input common-mode voltage is found by taking the average of the two voltages at the inputs to the comparator.

The LT1016 has an input voltage range from 1.25 V above the negative supply to 1.5 V below the positive supply. The AD8611 input voltage range extends down to the negative supply voltage to within 2 V of  $V_+$ . If the input common-mode voltage is exceeded, input signals must be shifted or attenuated to bring them into range, keeping in mind the note about source resistance in the Optimizing High Speed Performance section.

For example, an AD8611 powered from a 5 V single supply has its noninverting input connected to a 1 V peak-to-peak, high frequency signal centered around 2.3 V and its inverting input connected to a fixed 2.5 V reference voltage. The worst-case input common-mode voltage to the AD8611 is 2.65 V. This is well below the 3.0 V input common-mode voltage range to the comparator. Note that signals much greater than 3.0 V result in increased input currents and can cause the comparator to operate more slowly.

The input bias current to the AD8611 is 7  $\mu$ A maximum over temperature ( $-40^{\circ}\text{C}$  to  $+85^{\circ}\text{C}$ ). This is identical to the maximum input bias current for the LT1394, and half of the maximum  $I_B$  for the LT1016. Input bias currents to the AD8611 and LT1394 flow out from the comparator inputs, as opposed to the LT1016 whose input bias current flows into its inputs. Using low value resistors around the comparator and low impedance sources will minimize any potential voltage shifts due to bias currents.

The AD8611 is able to swing within 200 mV of ground and within 1.5 V of positive supply voltage. This is slightly more output voltage swing than the LT1016. The AD8611 also uses less current than the LT1016—5 mA as compared to 25 mA of typical supply current.

The AD8611 has a typical propagation delay of 4 ns, compared with the LT1394 and LT1016, whose propagation delays are typically 7 ns and 10 ns, respectively.

### MAXIMUM INPUT FREQUENCY AND OVERDRIVE

The AD8611 can accurately compare input signals up to 100 MHz with less than 10 mV of overdrive. The level of overdrive required increases with ambient temperature, with up to 50 mV of overdrive recommended for a 100 MHz input signal and an ambient temperature of  $+85^{\circ}\text{C}$ .

It is not recommended to use an input signal with a fundamental frequency above 100 MHz because the AD8611 could draw up to 20 mA of supply current and the outputs may not settle to a definite state. The device returns to its specified performance once the fundamental input frequency returns to below 100 MHz.

### OUTPUT LOADING CONSIDERATIONS

The AD8611 can deliver up to 10 mA of output current without increasing its propagation delay. The outputs of the device must not be connected to more than 40 TTL input logic gates or drive less than 400  $\Omega$  of load resistance.

The AD8611 output has a typical output swing between ground and 1 V below the positive supply voltage. Decreasing the output load resistance to ground lowers the maximum output voltage due to the increase in output current. Table 6 shows the typical output high voltage vs. load resistance to ground.

**Table 6. Maximum Output Voltage vs. Resistive Load**

Output Load to Ground	V+ – V <sub>OUT, HI</sub> (typ)
300 Ω	1.5 V
500 Ω	1.3 V
1 kΩ	1.2 V
10 kΩ	1.1 V
>20 kΩ	1.0 V

Connecting a 500 Ω to 2 kΩ pull-up resistor to V+ on the output helps increase the output voltage so that it is closer to the positive rail; in this configuration, however, the output voltage will not reach its maximum until 20 ns to 50 ns after the output voltage switches. This is due to the R-C time constant between the pull-up resistor and the output and load capacitances. The output pull-up resistor cannot improve propagation delay.

The AD8611 is stable with all values of capacitive load; however, loading an output with greater than 30 pF increases the propagation delay of that channel. Capacitive loads greater than 500 pF also create some ringing on the output wave. Table 7 shows propagation delay vs. several values of load capacitance. The loading on one output of the AD8611 does not affect the propagation delay of the other output.

**Table 7. Propagation Delay vs. Capacitive Load**

C <sub>L</sub> (pF)	t <sub>PD</sub> Rising (ns)	t <sub>PD</sub> Falling (ns)
<10	3.5	3.5
33	5	5
100	8	7
390	14.5	10
680	26	15

## USING THE LATCH TO MAINTAIN A CONSTANT OUTPUT

With the V<sub>CC</sub> supply at a nominal 5 V, the latch input to the AD8611/AD8612 can retain data at the output of the comparator. When the latch voltage goes high, the output voltage remains in its previous state, independent of changes in the input voltage.

The setup time for the AD8611/AD8612 is 0.5 ns and the hold time is 0.5 ns. Setup time is defined as the minimum amount of time the input voltage must remain in a valid state before the latch is activated for the latch to function properly. Hold time is defined as the amount of time the input must remain constant after the latch voltage goes high for the output to remain latched to its voltage.

The latch input is TTL and CMOS compatible, so a logic high is a minimum of 2.0 V and a logic low is a maximum of 0.8 V. The latch circuitry in the AD8611/AD8612 has no built-in hysteresis.

At or below approximately 4.1 V, the latch pin becomes unresponsive and must normally be tied low for low V<sub>CC</sub> operation.

## INPUT STAGE AND BIAS CURRENTS

The AD8611 and AD8612 each use a bipolar PNP differential input stage. This enables the input common-mode voltage range to extend from within 2.0 V of the positive supply voltage to 200 mV below the negative supply voltage. Therefore, using a single 5 V supply, the input common-mode voltage range is –200 mV to +3.0 V. Input common-mode voltage is the average of the voltages at the two inputs. For proper operation, the input common-mode voltage must be kept within the common-mode voltage range.

The input bias current for the AD8611/AD8612 is 4 μA, which is the amount of current that flows from each input of the comparator. This bias current goes to zero on an input that is high and doubles on an input that is low, which is a characteristic common to any bipolar comparator. Care must be taken in choosing resistances to be connected around the comparator because large resistors could significantly decrease the voltage due to the input bias current.

The input capacitance for the AD8611/AD8612 is typically 3 pF. This is measured by inserting a 5 kΩ source resistance in series with the input and measuring the change in propagation delay.

## USING HYSTERESIS

Hysteresis can easily be added to a comparator through the addition of positive feedback. Adding hysteresis to a comparator offers an advantage in noisy environments where it is undesirable for the output to toggle between states when the input signal is close to the switching threshold. Figure 24 shows a simple method for configuring the AD8611 or AD8612 with hysteresis.

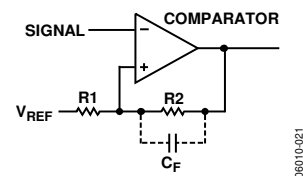


Figure 24. Configuring the AD8611/AD8612 with Hysteresis

In Figure 24, the input signal is connected directly to the inverting input of the comparator. The output is fed back to the noninverting input through R1 and R2. The ratio of R1 to R1 + R2 establishes the width of the hysteresis window, with V<sub>REF</sub> setting the center of the window, or the average switching voltage. The QA or QB output switches low when the input voltage is greater than V<sub>HI</sub>, and does not switch high again until the input voltage is less than V<sub>LO</sub>, as given in Equation 1:

$$V_{HI} = \left( V_+ - 1.5 V_{REF} \right) \frac{R1}{R1 + R2} + V_{REF} \quad (1)$$

$$V_{LO} = V_{REF} \times \frac{R2}{R1 + R2}$$

where V<sub>+</sub> is the positive supply voltage.

The capacitor  $C_F$  is optional and can be added to introduce a pole into the feedback network. This has the effect of increasing the amount of hysteresis at high frequencies, which is useful when comparing relatively slow signals in high frequency noise environments. At frequencies greater than  $f_P$ , the hysteresis window approaches  $V_{HI} = V+ - 1.5 V$  and  $V_{LO} = 0 V$ . For frequencies less than  $f_P$ , the threshold voltages remain as in Equation 1.

**CLOCK TIMING RECOVERY**

Comparators are often used in digital systems to recover clock timing signals. High speed square waves transmitted over any distance, even tens of centimeters, can become distorted due to stray capacitance and inductance. Poor layout or improper termination can also cause reflections on the transmission line, further distorting the signal waveform. A high speed comparator can recover the distorted waveform while maintaining a minimum of delay.

Figure 25 shows  $V_{OUT}$  vs.  $V_{IN}$  as the AD8611 recovers a 65 MHz, 100 mV peak-to-peak distorted clock signal into a 4 V peak-to-peak square wave. The lower trace is the input to the AD8611, and the upper trace is the QA or QB output from the comparator. The AD8611 is powered from a 5 V single supply.

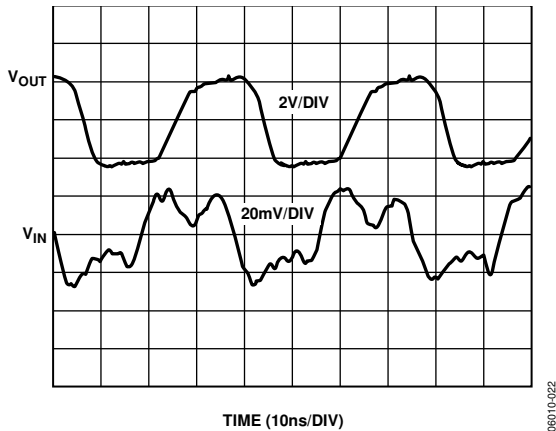


Figure 25. Using the AD8611 to Recover a Noisy Clock Signal

**A 5 V, HIGH SPEED WINDOW COMPARATOR**

A window comparator circuit detects when a signal is between two fixed voltages. The AD8612 can create a high speed window comparator, as shown in Figure 26. In this example, the reference window voltages are set as:

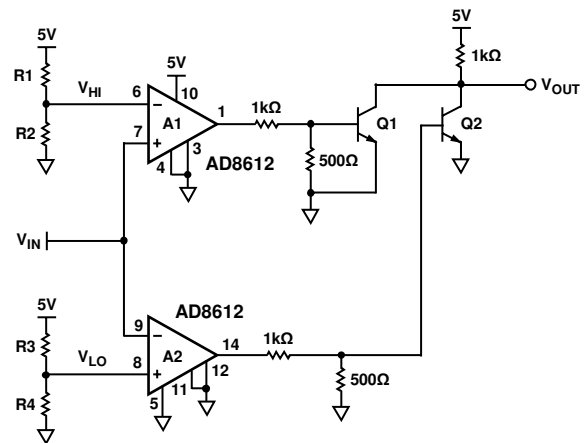
$$V_{HI} = \frac{R2}{R1 + R2} \quad V_{LO} = \frac{R4}{R3 + R4}$$

The output of the A1 comparator goes high when the input signal exceeds  $V_{HI}$ , and the output of A2 goes high only when  $V_{IN}$  drops below  $V_{LO}$ . When the input voltage is between  $V_{HI}$  and  $V_{LO}$ , both comparator outputs are low, turning off both Q1 and Q2, thus driving  $V_{OUT}$  to a high state. If the input signal goes outside of the reference voltage window,  $V_{OUT}$  goes low.

To ensure a minimum of switching delay, the use of high speed transistors is recommended for Q1 and Q2. Using the AD8612 with 2N3960 transistors provides a total propagation delay from  $V_{IN}$  to  $V_{OUT}$  of less than 10 ns.

**Table 8. Window Comparator Output States**

$V_{OUT}$	Input Voltage
$\approx 200 mV$	$V_{IN} < V_{LO}$
+5 V	$V_{LO} < V_{IN} < V_{HI}$
$\approx 200 mV$	$V_{IN} > V_{HI}$



- NOTES**  
 1. Q1, Q2 = 2N3960.  
 2. PINS 2 AND 13 ARE NO CONNECTS.

Figure 26. A High Speed Window Comparator

**SPICE Model**

\* AD8611 SPICE Macro-Model Typical Values

\* 1/2000, Ver. 1.0

\* TAM/ADSC

\*

\* Node assignments

```

*           non-inverting input
*           |           inverting input
*           |           |           positive supply
*           |           |           |           negative supply
*           |           |           |           |           Latch
*           |           |           |           |           |           DGND
*           |           |           |           |           |           |           Q
*           |           |           |           |           |           |           |           QNOT
*           |           |           |           |           |           |           |           |
.SUBCKT AD8611 1 2 99 50 80 51 45 65

```

\*

\* INPUT STAGE

\*

\*

```

Q1 4 3 5 PIX
Q2 6 2 5 PIX
IBIAS 99 5 800E-6
RC1 4 50 1E3
RC2 6 50 1E3
CL1 4 6 3E-13
CIN 1 2 3E-12
VCM1 99 7 DC 1.9
D1 5 7 DX
EOS 3 1 POLY(1) (31,98) 1E-3 1

```

\*

\* Reference Voltages

\*

```

EREF 98 0 POLY(2) (99,0) (50,0) 0 0.5 0.5
RREF 98 0 100E3

```

\*

\* CMRR = 66dB, ZERO AT 1 kHz

\*

ECM1	30	98	POLY(2)	(1,98)	(2,98)	0	0.5	0.5
RCM1	30	31	10E3					
RCM2	31	98	5					
CCM1	30	31	15.9E-9					

\*  
\* Latch Section

\*

RX	80	51	100E3					
E1	10	98	(4,6)	1				
S1	10	11	(80,51)	SLATCH1				
R2	11	12	1					
C3	12	98	5	4E-12				
E2	13	98	(12,98)	1				
R3	12	13	500					

\*  
\* Power Supply Section

\*

GSY1	99	52	POLY(1)	(99,50)	4E-3	-2	6E-4
GSY2	52	50	POLY(1)	(99,50)	3	7E-3	-.6E-3
RSY	52	51	10				

\*  
\* Gain Stage Av = 250 fp=100 MHz

\*

G2	98	20	(12,98)	0.25
R1	20	98	1000	
C1	20	98	10E-13	
E3	97	0	(99,0)	1
E4	52	0	(51,0)	1
V1	97	21	DC	0.8
V2	22	52	DC	0.8
D2	20	21	DX	
D3	22	20	DX	

\*  
\* Q Output

\*

Q3	99	41	46	NOX
----	----	----	----	-----

Q4	47	42	51	NOX
RB1	43	41	2000	
RB2	40	42	2000	
CB1	99	41	0.5E-12	
CB2	42	51	1E-12	
RO1	46	44	1	
D4	44	45	DX	
RO2	47	45	500	
EO1	97	43	(20, 51)	1
EO2	40	51	(20, 51)	1

\*

\* Q NOT Output

\*

Q5	99	61	66	NOX
Q6	67	62	51	NOX
RB3	63	61	2000	
RB4	60	62	2000	
CB3	99	61	0	5E-12
CB4	62	51	1E-12	
RO3	66	64	1	
D5	64	65	DX	
RO4	67	65	500	
EO3	63	51	(20, 51)	1
EO4	97	60	(20, 51)	1

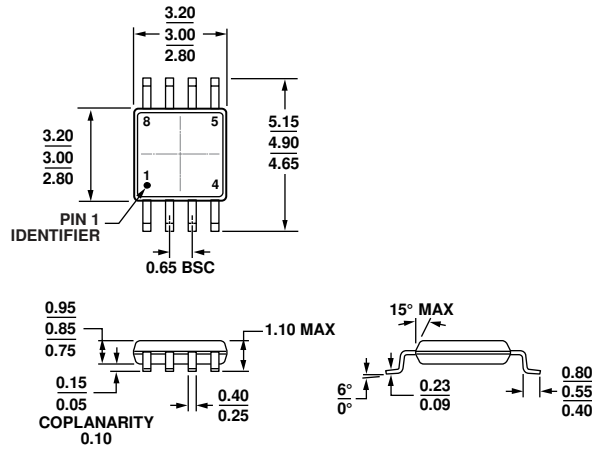
\*

\* MODELS

\*

```
.MODEL PIX PNP (BF=100, IS=1E-16)
.MODEL NOX NPN (BF=100, VAF=130, IS=1E-14)
.MODEL DX D (IS=1E-14)
.MODEL SLATCH1 VSWITCH (ROFF=1E6, RON=500,
+VOFF=2.1, VON=1.4)
.ENDS AD8611
```

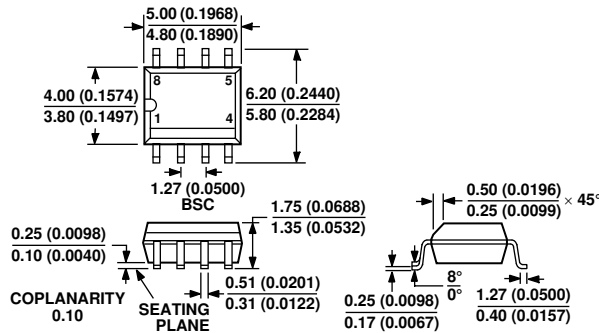
OUTLINE DIMENSIONS



COMPLIANT TO JEDEC STANDARDS MO-187-AA

Figure 27. 8-Lead Mini Small Outline Package [MSOP] (RM-8)

Dimensions shown in millimeters

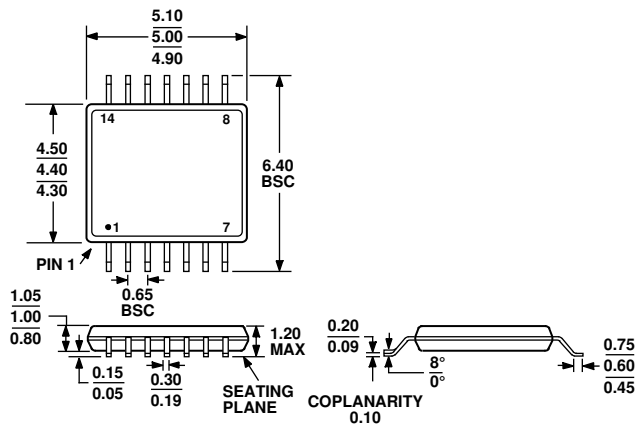


COMPLIANT TO JEDEC STANDARDS MS-012-AA

CONTROLLING DIMENSIONS ARE IN MILLIMETERS; INCH DIMENSIONS (IN PARENTHESES) ARE ROUNDED-OFF MILLIMETER EQUIVALENTS FOR REFERENCE ONLY AND ARE NOT APPROPRIATE FOR USE IN DESIGN.

Figure 28. 8-Lead Standard Small Outline Package [SOIC\_N] Narrow Body (R-8)

Dimensions shown in millimeters and (inches)



COMPLIANT TO JEDEC STANDARDS MO-153-AB-1

Figure 29. 14-Lead Thin Shrink Small Outline Package [TSSOP] (RU-14)

Dimensions shown in millimeters



**ORDERING GUIDE**

<b>Model<sup>1</sup></b>	<b>Temperature Range</b>	<b>Package Description</b>	<b>Package Option</b>	<b>Branding</b>
AD8611ARMZ-REEL	-40°C to +85°C	8-Lead Mini Small Outline Package [MSOP]	RM-8	G1A
AD8611ARMZ-R2	-40°C to +85°C	8-Lead Mini Small Outline Package [MSOP]	RM-8	G1A
AD8611AR	-40°C to +85°C	8-Lead Standard Small Outline Package [SOIC_N]	R-8	
AD8611ARZ	-40°C to +85°C	8-Lead Standard Small Outline Package [SOIC_N]	R-8	
AD8611ARZ-REEL	-40°C to +85°C	8-Lead Standard Small Outline Package [SOIC_N]	R-8	
AD8611ARZ-REEL7	-40°C to +85°C	8-Lead Standard Small Outline Package [SOIC_N]	R-8	
AD8612ARUZ	-40°C to +85°C	14-Lead Thin Shrink Small Outline Package [TSSOP]	RU-14	
AD8612ARUZ-REEL	-40°C to +85°C	14-Lead Thin Shrink Small Outline Package [TSSOP]	RU-14	

<sup>1</sup> Z = RoHS Compliant Part.

**NOTES**

**NOTES**

**NOTES**